

Application Note

AN- EVALQRC-ICE2QR0665

40W20V Evaluation Board with Quasi-Resonant CoolSET[®] ICE2QR0665

Power Management & Supply



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1 Content

This application note is a description of 40W switching mode power supply evaluation board designed in a quasi resonant flyback converter topology using ICE2QR0665 Quasi-resonant CoolSET®. The target application of ICE2QR0665 are for set-top box, portable game controller, DVD player, netbook adapter and auxiliary power supply for LCD TV, etc. With the CoolMOS® integrated in this IC, it greatly simplifies the design and layout of the PCB. Due to valley switching, the turn on voltage is reduced and this offers higher conversion efficiency comparing to hard-switching flyback converter. With the DCM mode control, the reverse recovery problem of secondary rectify diode is relieved. And for its natural frequency jittering with line voltage, the EMI performance is better. Infineon's digital frequency reduction technology enables a quasi-resonant operation till very low load. As a result, the system efficiency, over the entire load range, is significantly improved compared to conventional free running quasi resonant converter implemented with only maximum switching frequency limitation at light load. In addition, numerous adjustable protection functions have been implemented in ICE2QR0665 to protect the system and customize the IC for the chosen application. In case of failure modes, like open control-loop/over load, output overvoltage, and transformer short winding, the device switches into **Auto Restart Mode** or **Latch-off Mode**. By means of the cycle-by-cycle peak current limitation plus foldback point correction, the dimension of the transformer and current rating of the secondary diode can both be optimized. Thus, a cost effective solution can be easily achieved.

2 Evaluation Board



Figure 1-EVALSQ-40W-ICE2QR0665

3 List of Features

Industry first IC in DIP8 package with 40W maximum output power
650V avalanche rugged CoolMOS® with built in depletion startup cell
Quasi-resonant operation
Digital frequency reduction with decreasing load
Cycle-by-cycle peak current limitation with foldback point correction
Built-in digital soft-start
Direct current sensing with internal Leading Edge Blanking Time
VCC under voltage protection: IC stop operation, recover with softstart
VCC over voltage protection: IC stop operation, recover with softstart
Openloop/Overload protection: Auto Restart
Output overvoltage protection: Latch-off with adjustable threshold
Short-winding protection: Latch-off
Over temperature protection: Autorestart

4 Technical Specifications

Input voltage	85Vac~265Vac
Input frequency	50Hz, 60Hz
Output voltage and current	20V 2A
Output power	40W
Efficiency	>86% at full load
Standby power	<100mW@no load
Minimum switching frequency at full load, minimum input voltage	40kHz

5 Circuit Description

5.1 Mains Input and Rectification

The AC line input side comprises the input fuse F1 as overcurrent protection. The X2 Capacitors C1, C2 and Choke L1 form a main filter to minimize the feedback of RFI into the main supply. After the bridge rectifier BR1, together with a smoothing capacitor C3, provide a voltage of 70VDC to 380 VDC depending on mains input voltage. A 2.5 Ω NTC resistor is placed in series with input to limit the initial peak inrush current whenever the power supply is switched on when C3 is fully discharged.

5.2 Integrated MOSFET and PWM Control

ICE2QR0665 is comprised of a power MOSFET and the quasi-resonant controller; this integrated solution greatly simplifies the circuit layout and reduces the cost of PCB manufacturing. The PWM switch-on is determined by the zero-crossing input signal and the value of the up/down counter. The PWM switch-off is determined by the feedback signal V_{FB} and the current sensing signal V_{CS} . ICE2QR0665 also performs all necessary protection functions in flyback converters. Details about the information mentioned above are illustrated in the product datasheet.

5.3 Snubber Network

A snubber network R1, C4 and D1 dissipate the energy of the leakage inductance and suppress ringing on the SMPS transformer. Due to the resonant capacitor C10 paralleled to MOSFET drain source pin, the overshoot is relatively smaller than fixed frequency flyback converter. Thus the snubber resistor can be used with a larger one which will reduce the snubber loss.

5.4 Output Stage

On the secondary side, 20V output, the power is coupled out via a dual schottky diode D3. The capacitors C11 and C16 provide energy buffering followed by the L-C filters L2 and C12 to reduce the output ripple and prevent interference between SMPS switching frequency and line frequency considerably. Storage capacitors C11 and C16 are designed to have an internal resistance (ESR) as small as possible. This is to minimize the output voltage ripple caused by the triangular current.

5.5 Feedback Loop

For feedback, the output is sensed by the voltage divider of R10, R11 and R12 and compared to TL431 internal reference voltage. C15, C14 and R8 comprise the compensation network. The output voltage of TL431 is converted to the current signal via optocoupler IC2 and two resistors R6 and R7 for regulation control.

6 Circuit Operation

6.1 Startup Operation

Since there is a built-in startup cell in the ICE2QR0665, there is no need for external start up resistor, which can improve standby performance significantly.

When VCC reaches the turn on voltage threshold 18V, the IC begins with a soft start. The soft-start implemented in ICE2QR0665 is a digital time-based function. The preset soft-start time is 12ms with 4 steps. If not limited by other functions, the peak voltage on CS pin will increase step by step from 0.32V to 1V finally. After IC turns on, the Vcc voltage is supplied by auxiliary windings of the transformer.

6.2 Normal Mode Operation

The secondary output voltage is built up after startup. The secondary regulation control is adopted with TL431 and optocoupler. The compensation network C14, C15 and R8 constitutes the external circuitry of the error amplifier of TL431. This circuitry allows the feedback to be precisely controlled with respect to dynamically varying load conditions, therefore providing stable control.

6.3 Primary side peak current control

The MOSFET drain source current is sensed via external resistor R5 and R5A. Since ICE2QR0665 is a current mode controller, it would have a cycle-by-cycle primary current and feedback voltage control which can make sure the maximum power of the converter is controlled in every switching cycle.

6.4 Digital Frequency Reduction

During normal operation, the switching frequency for ICE2QR0665 is digitally reduced with decreasing load. At light load, the MOSFET will be turned on not at the first minimum drain-source voltage time, but on the n^{th} . The counter is in range of 1 to 7, which depends on feedback voltage in a time-base. The feedback voltage decreases when the output power requirement decreases, and vice versa. Therefore, the counter is set by monitoring voltage V_{FB} . The counter will be increased with low V_{FB} and decreased with high V_{FB} . The thresholds are preset inside the IC.

6.5 Burst Mode Operation

At light load condition, the SMPS enters into Active Burst Mode. At this stage, the controller is always active but the Vcc must be kept above the switch off threshold. During active burst mode, the efficiency increase significantly and at the same time it supports low ripple on V_{out} and fast response on load jump.

For determination of entering Active Burst Mode operation, three conditions apply:

- .the feedback voltage is lower than the threshold of V_{FBEB} (1.3V). Accordingly, the peak current sense voltage across the shunt resistor is 0.18;
- .the up/down counter is 7;
- .and a certain blanking time (t_{BEB}).

Once all of these conditions are fulfilled, the Active Burst Mode flip-flop is set and the controller enters Active Burst Mode operation. This multi-condition determination for entering Active Burst Mode operation prevents mistripping of entering Active Burst Mode operation, so that the controller enters Active Burst Mode operation only when the output power is really low during the preset blanking time.

During active burst mode, the maximum current sense voltage is reduced from 1V to 0.34V so as to reduce the conduction loss and the audible noise. At the burst mode, the FB voltage is changing like a sawtooth between 3.0 and 3.6V.

The feedback voltage immediately increases if there is a high load jump. This is observed by one comparator. As the current limit is 34% during Active Burst Mode a certain load is needed so that feedback voltage can exceed VLB (4.5V). After leaving active burst mode, maximum current can now be provided to stabilize V_{O} . In addition, the up/down counter will be set to 1 immediately after leaving Active Burst Mode. This is helpful to decrease the output voltage undershoot

7 Protection Features

7.1 Vcc under voltage and over voltage protection

During normal operation, the VCC voltage is continuously monitored. When the Vcc voltage falls below the under voltage lock out level (VCCoff) or the Vcc voltage increases up to VCCovp, the IC will enter into autorestart mode.

7.2 Foldback point protection

For a quasi-resonant flyback converter, the maximum possible output power is increased when a constant current limit value is used for all the mains input voltage range. This is usually not desired as this will increase additional cost on transformer and output diode in case of output over power conditions.

The internal fold back protection is implemented to adjust the Vcs voltage limit according to the bus voltage. Here, the input line voltage is sensed using the current flowing out of ZC pin, during the MOSFET on-time. As the result, the maximum current limit will be lower at high input voltage and the maximum output power can be well limited versus the input voltage.

7.3 Open loop/over load protection

In case of open control loop, feedback voltage is pulled up with internally block. After a fixed blanking time 30ms, the IC enters into auto restart mode. In case of secondary short-circuit or overload, regulation voltage V_{FB} will also be pulled up, same protection is applied and IC will auto restart.

7.4 Adjustable output overvoltage protection

During off-time of the power switch, the voltage at the zero-crossing pin ZC is monitored for output overvoltage detection. If the voltage is higher than the preset threshold 3.7V for a preset period 100 μ s, the IC is latched off.

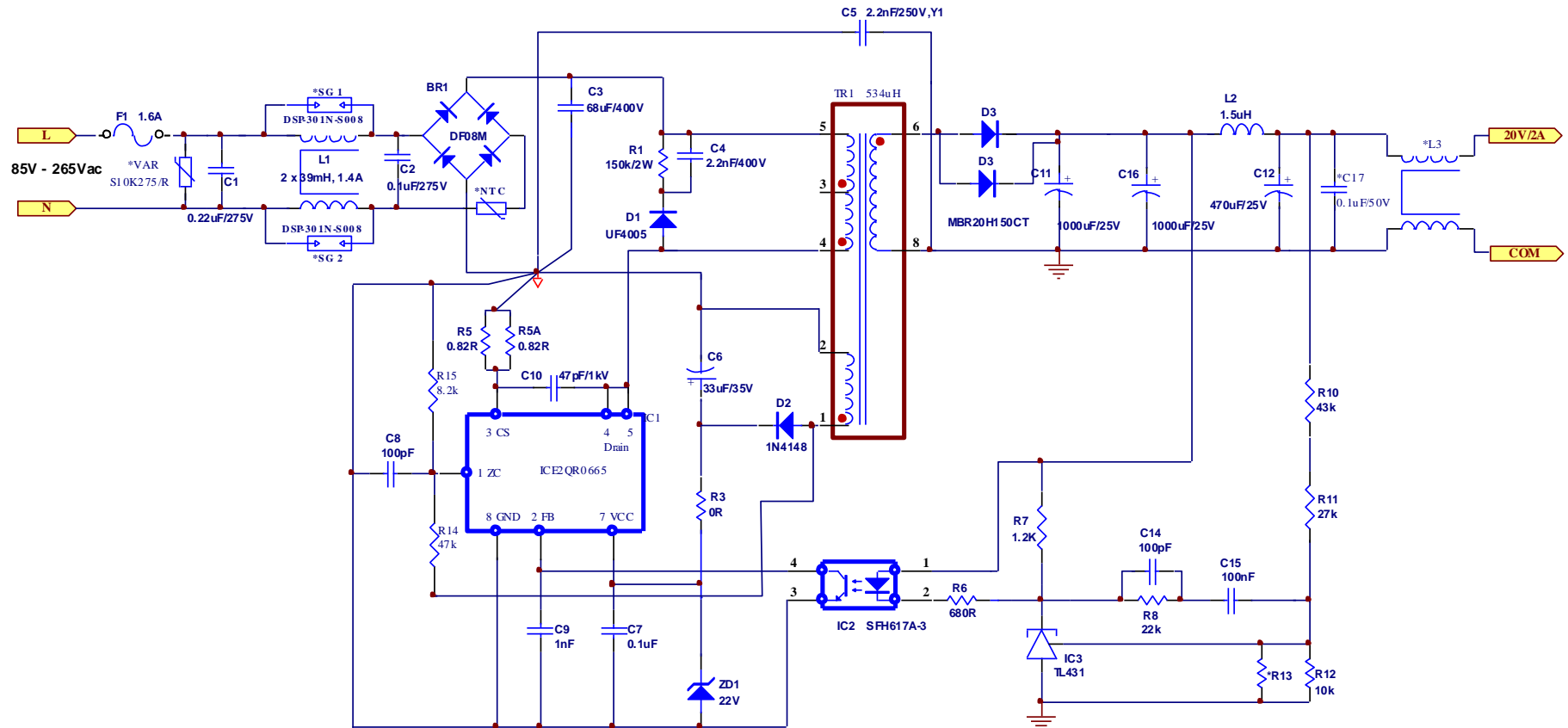
7.5 Short winding protection

The source current of the MOSFET is sensed via two shunt resistors R5 and R5A in parallel. If the voltage at the current sensing pin is higher than the preset threshold V_{CSSW} of 1.68V during the on-time of the power switch, the IC is latched off. This constitutes a short winding protection. To avoid an accidental latch off, a spike blanking time of 190ns is integrated in the output of internal comparator.

7.6 Auto restart for over temperature protection

The IC has a built-in over temperature protection function. When the controller's temperature reaches 140 °C, the IC will shut down switch and enters into autorestart. This can protect power MOSFET from overheated.

8 Circuit diagram



40W 20V SMPS Demoboard with ICE2QR0665(V0.2)

Figure 2 – Schematics

8.1 PCB Topover layer

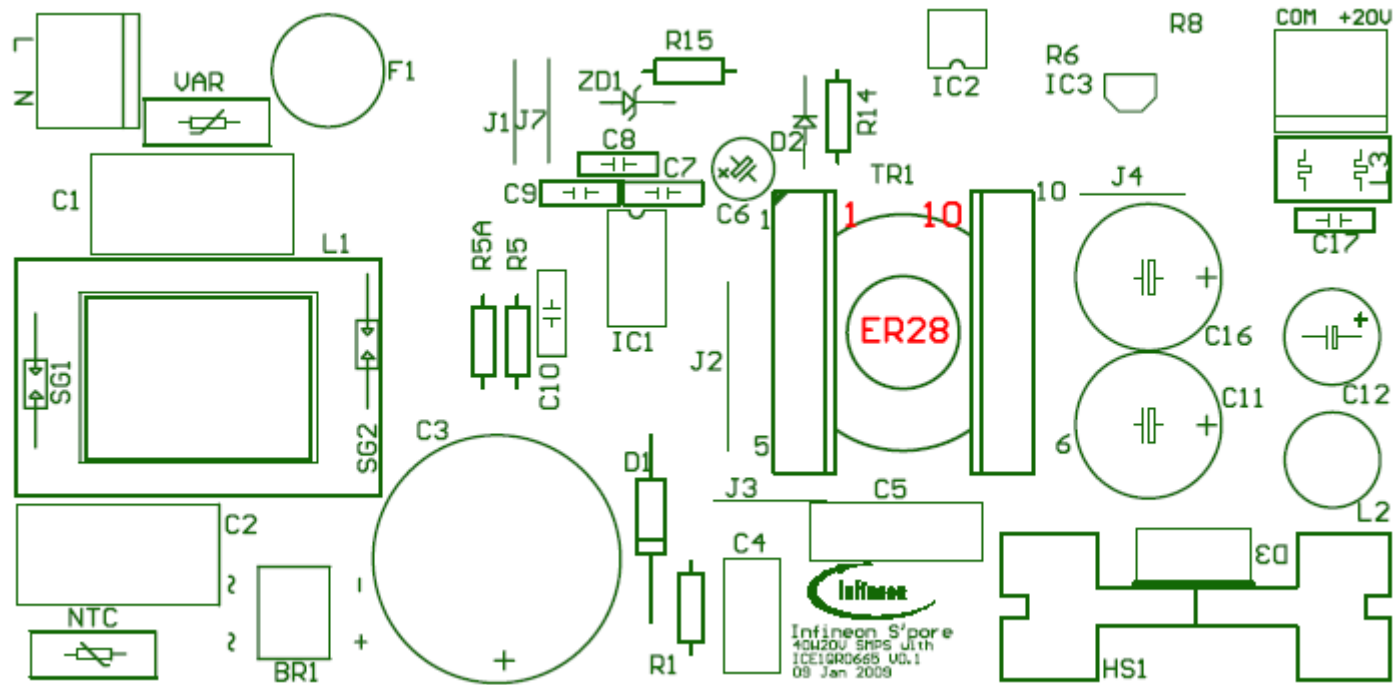


Figure 3 –Component Legend – View from topside

8.2 PCB Bottom Layer

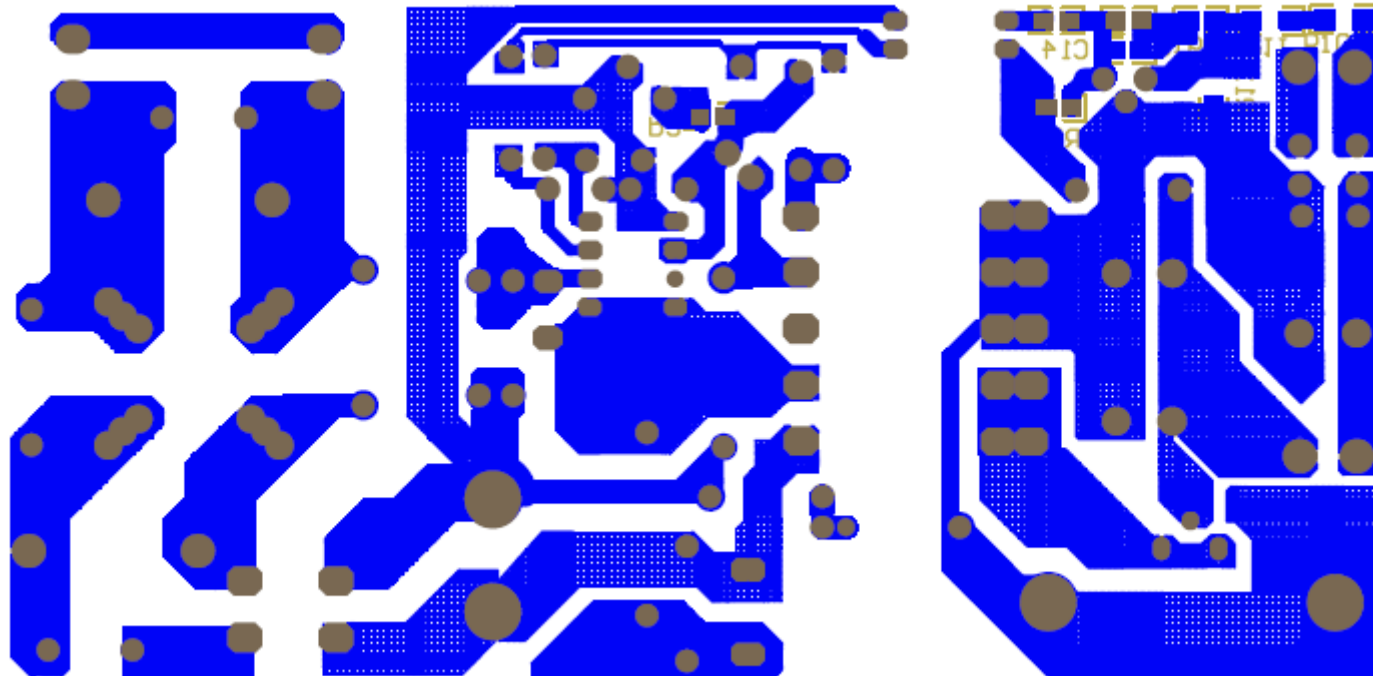


Figure 4 Solder side copper – View from bottom side

9 Component List

Table 1– Component List

Items	Designator	Part Type	Part no.	Manufacturer
1	BR1	1.5A/800V	DF08M	Vishay
2	NTC	2.5Ω S236	B57236S0259M000	Epcos
3	C1	0.22μF/275Vac X2	B32922C3224K000	Epcos
4	C2	0.1μF/275Vac X2	B32922C3104K000	Epcos
5	C3	68μF/400V	B43501A9686M000	Epcos
6	C4	2.2nF/400V	B32529C8222K000	Epcos
7	C5	2.2nF/250V, Y1	DE1E3KX222MA4BL01	Murata
8	C6	33μF/35V	B41851A7336M000	Epcos
9	C7	0.1μF	RPER71H104K2K1A03B	Murata
10	C8	100pF		
11	C9	1nF	RPER71H102K2K1A03B	Murata
12	C10	47pF/1000V		
13	C11	1000μF/25V		
14	C12	470μF/25V		
15	C14	100pF(0805)		
16	C15	100nF(0805)		
17	C16	1000μF/25V		
18	D1	UF4005	UF4005	Vishay
19	D2	1N4148		
20	D3	20A/150V	MBR20H150CT	Vishay
21	F1	1.6A Fuse		
22	FB1	Ferrite Bead		
23	IC1	ICE2QR0665		Infineon
24	IC2	SFH617A-3		
25	IC3	TL431		
26	J1~J7	Jumper		
27	L1	2X39mH,1.4A	B82734R2142B030	Epcos
28	L2	1.5μH		
29	R1	150kΩ/2W		
30	R3	0Ω, (SMD 0805)		
31	R5	0.82Ω(0.5W, 1%)		
32	R5A	0.82Ω(0.5W, 1%)		
33	R6	680Ω(SMD 0805)		
34	R7	1.2kΩ(SMD 0805)		
35	R8	22kΩ(SMD 0805)		
36	R10	43kΩ,0.1% (1206)		
37	R11	27kΩ,1%(1206)		
38	R12	10kΩ(1%)(1206)		
39	R14	47kΩ		
40	R15	8.2kΩ		
41	TR1	534μH	PC40EER28-Z	TDK
42	ZD1	22V		

10 Transformer Construction

Core and material: PC40EER28-Z

Bobbin: Horizontal Version, BEER-28-1110CP

Primary Inductance, $L_p=534\mu\text{H}$, measured between pin 5 and pin 4 (Gapped to Inductance)

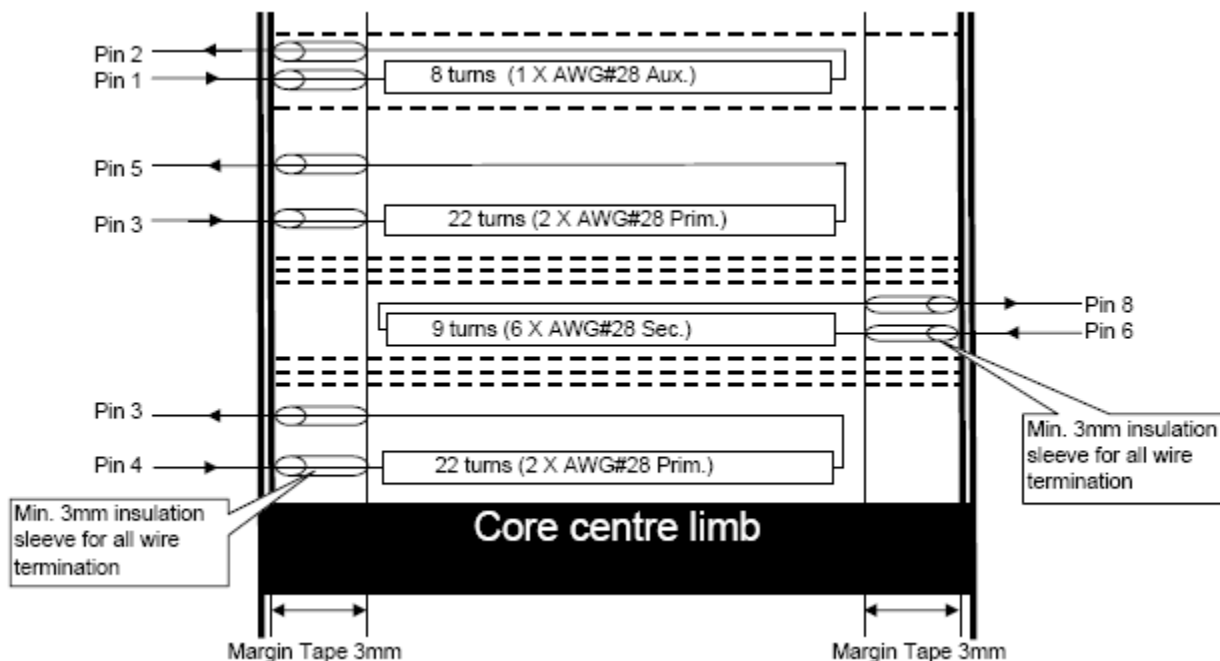


Figure 5 – Transformer structure

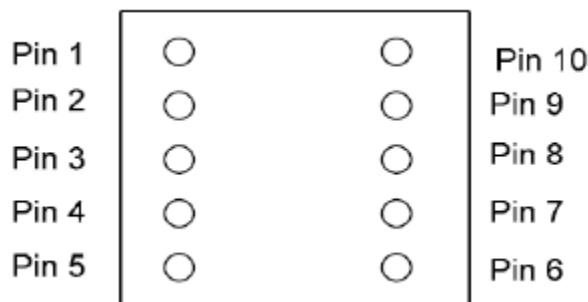


Figure 6 – Transformer complete – top view

Table 2 wire gauge used of the transformer windings

Start	Stop	No. of turns	Wire size	Layer
1	2	8	1XAWG#28	Auxiliary
3	5	22	2XAWG#28	$\frac{1}{2}$ Primary
6	8	9	6XAWG#28	Secondary
4	3	22	2XAWG#28	$\frac{1}{2}$ Primary

11 Test Results

11.1 Efficiency and standby performance

Table 3 – Efficiency vs. AC line voltage

Input voltage(Vac)	Input power(W)	Vo(V)	Io(A)	Po(W)	Efficiency(%)
90	11.314	19.88	0.5037	10.01356	88.51
90	22.664	19.87	1.0025	19.91968	87.89
90	33.923	19.86	1.5006	29.80192	87.85
90	46.002	19.86	2.0037	39.79348	86.50
100	11.281	19.88	0.5037	10.01356	88.76
100	22.51	19.87	1.0025	19.91968	88.49
100	33.744	19.86	1.5006	29.80192	88.32
100	45.452	19.86	2.0037	39.79348	87.55
230	11.335	19.88	0.5037	10.01356	88.34
230	22.129	19.87	1.0025	19.91968	90.02
230	33.052	19.86	1.5006	29.80192	90.17
230	44.091	19.86	2.0037	39.79348	90.25

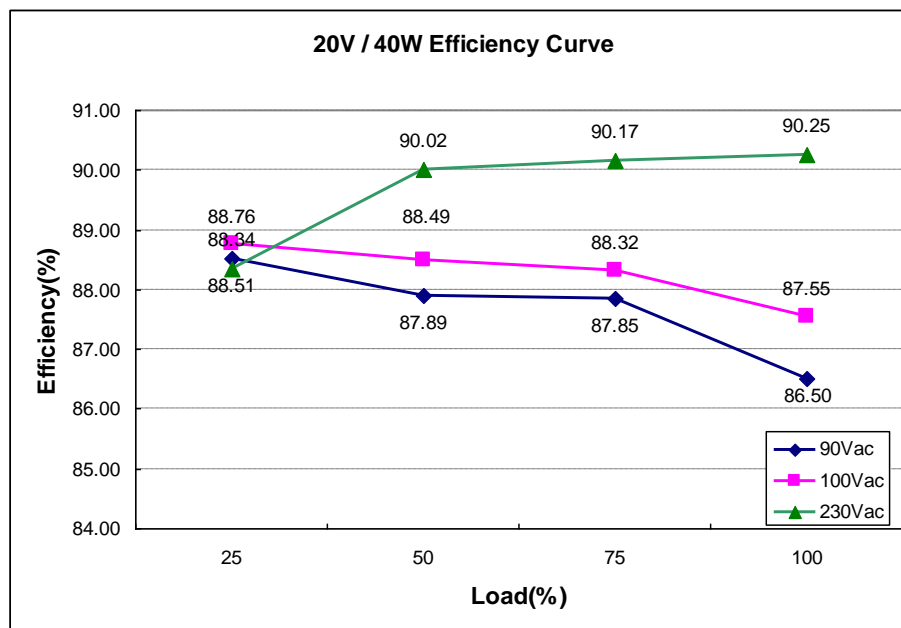


Figure 7 – Efficiency vs. AC line voltage

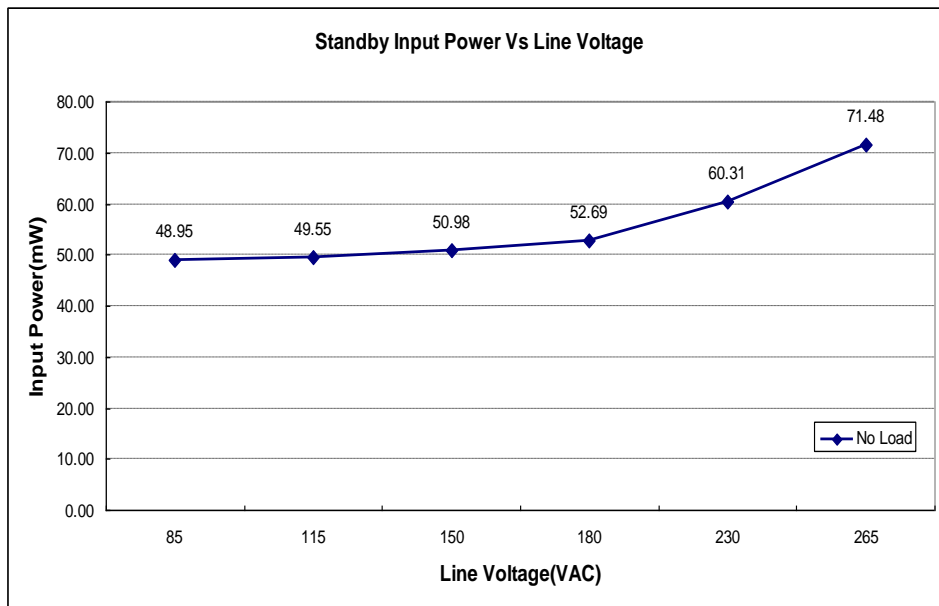


Figure 8 Standby input power vs AC line voltage

11.2 EMI test results

The conducted EMI was measured by Schaffner (SMR4503) under test standard EN55022 or CISPR22 Class B. The demo board was set up at 36W with the input voltage at 115Vac and 230Vac. The Red curve(upper one) is the Quasi Peak data and the Green cuve(lower one) is the Average data. Both of them can meet the regulations.

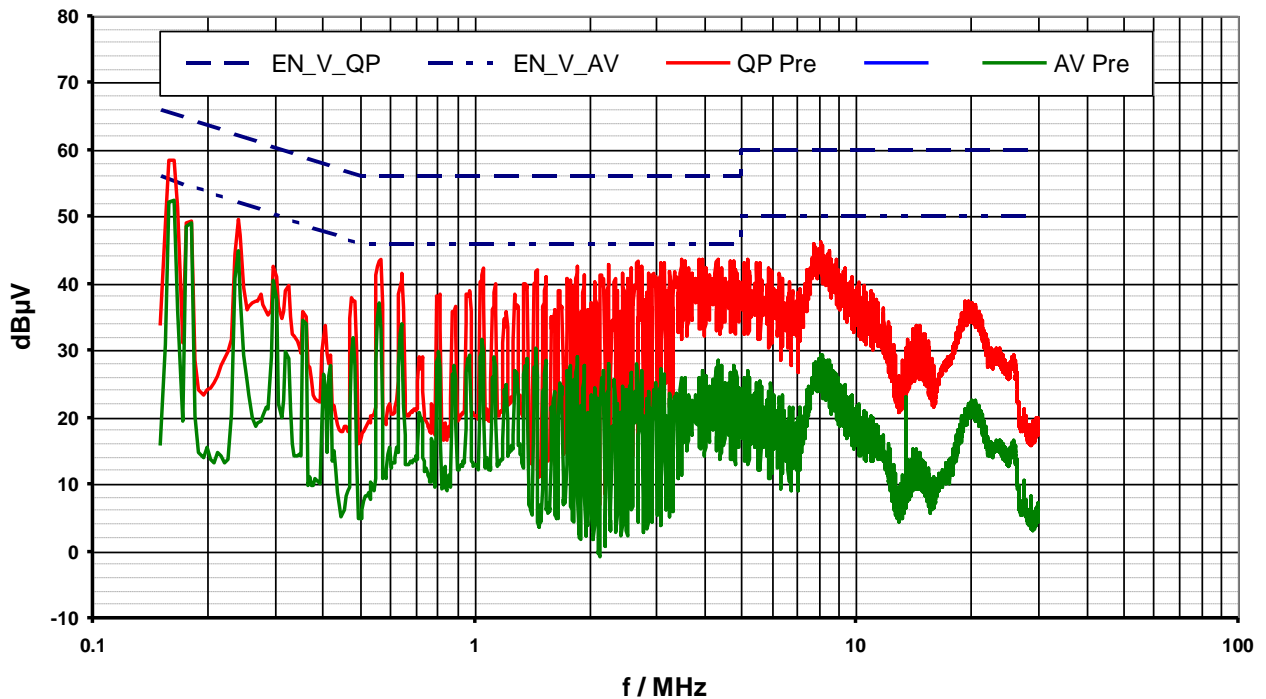


Figure 9 230V Line results

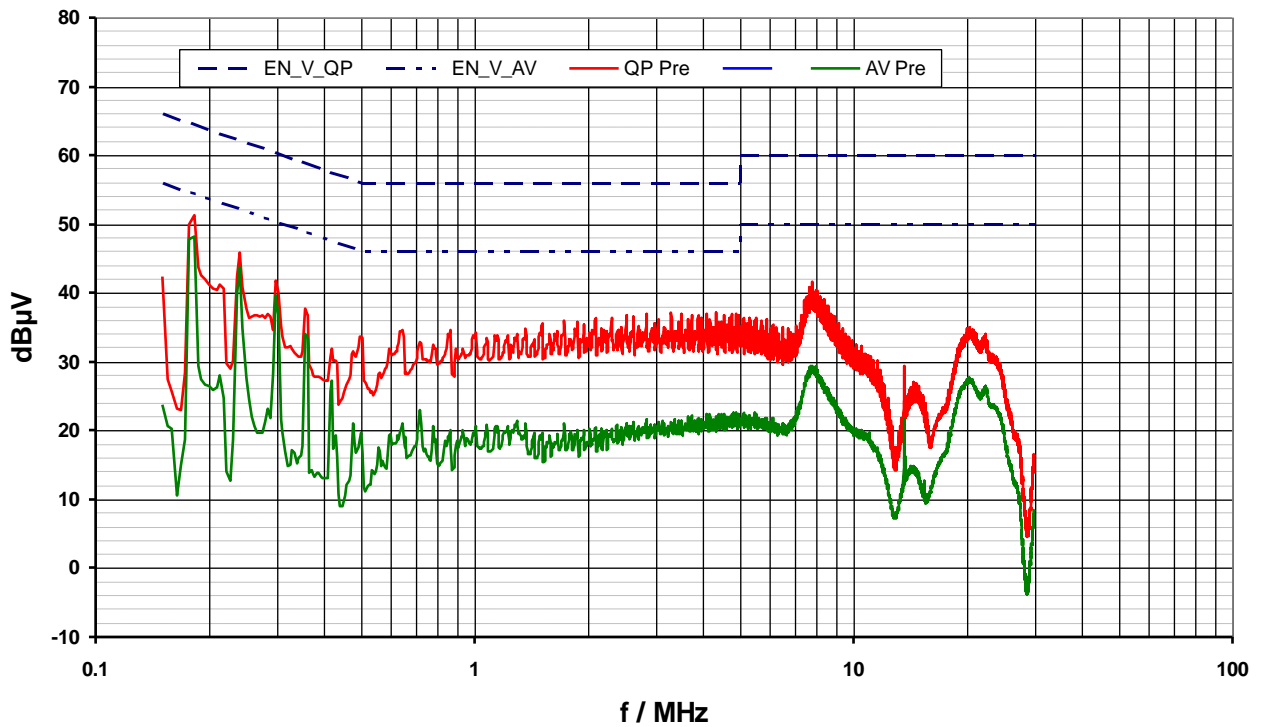


Figure 10 115V line results

12 References

- [1] ICE2QS01 datasheet, Infineon Technologies AG, 2006
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